An Efficiency-Improved Tightly Coupled Dipole Reflectarray Antenna Using Variant-Coupling-Capacitance Method

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ABSTRACT
In this paper, a tightly coupled dipole reflectarray antenna as well as a variant-coupling-capacitance method to improve the antenna aperture efficiency is presented. Tightly coupled elements and true-time-delay lines are employed in the design of a wideband reflectarray. The proposed reflectarray can operate from 2 GHz to 5 GHz with the gain varying from 11.3 dBi to 21 dBi. Moreover, we propose a variant-coupling-capacitance method to improve the reflectarray aperture efficiency at lower frequency. By changing the coupling capacitance between neighboring elements according to their positions in the reflecting surface, a more linear equivalent distance delay line is achieved. Hence, phase error is reduced. According to measurement, the reflectarray gain in 2 GHz using the proposed method is increased by 3 dBi compared with the previous design. Aperture efficiency in 2 GHz is improved by 21.6%.

INDEX TERMS
Reflectarray, tightly coupled antenna, wideband, variant coupling capacitance.

I. INTRODUCTION
Reflectarray (RA) antennas are a new generation of high-gain antennas thanks to their distinguishable electrical and mechanical characteristics. RA antennas combine merits of both reflectors and printed arrays as well as offering alternative design with low profile and low mass features [1], [2]. In comparison with reflector antennas, RA antennas are easy to manufacture and install due to their flat structures. Compared with printed arrays, RA antennas eliminate the loss from feedline networks and phase adjustment networks as reflectarray has usually one feed antenna, and the elements embed phase altering structures to achieve plane wave on the aperture surface [3].

Although RA antennas outweigh many kinds of antennas in terms of various favorable features, they suffer from the disadvantage of narrow bandwidth. The main factors that restrain bandwidth are the bandwidth of the reflectarray elements and the differential spatial phase delay [4]. Many approaches have been adopted to broaden the bandwidth. In terms of improving the unit cell bandwidth performance, multi-resonant elements [5], [6], multilayer elements [2], [7], spline shaped unit cell [8], and subwavelength element [9] are employed. In order to compensate the differential spatial phase delay caused by different paths from the feed to different elements, true-time-delay techniques are used in [10], [11]. Besides these methods, a phase synthesis approach is developed to increase bandwidth independent of the element frequency behavior [12].

Recently another approach proposed by [13] utilizes tightly coupled dipole reflectarray elements to increase bandwidth to a great extent. Tightly coupled antenna is first proposed by Ben Munk [14] based on Wheeler’s current sheet theory [15]. The coupling capacitance between elements is exploited to improve bandwidth performance. Researchers from Kent University firstly applied tightly coupled theory into reflectarray design and achieved the bandwidth of 103%. Besides reflectarray, tightly coupled elements are also utilized to design transmittarrays [16].

In this paper, we present a tightly coupled dipole reflectarray antenna (TCDRA). Section II demonstrates the design basis of a TCDRA. The proposed TCDRA operates from 2 GHz to 5 GHz with the gain varying from 11.3 dBi to 21 dBi. However, though the reflectarray has a wider
bandwidth than most of the existed reflectarrays, in lower frequency the gain is relatively low. This is because in lower frequency the behaviors of the reflecting elements deviate from the designed value and phase error becomes greater. Therefore, in Section III we propose a variant-coupling-capacitance (VCC) method to increase the gain in lower frequency. By changing the coupling capacitance between neighboring unit cells according to their positions in the reflecting surface, the linearity of phase delay line improves in the objective frequency. And the difference between the objective frequency design line and the ultimate design line is reduced. As a result, the objective frequency gain is increased. The model is simulated and fabricated to verify the design. Measurement results in Section IV show that the variant-coupling-capacitance tightly coupled dipole reflectarray antenna (VTCDRA) gain is increased by 3 dBi in 2 GHz. The modified antenna gain varies from 14.4 dBi to 21.9 dBi within the working frequency of 2 GHz to 5 GHz. The cross polarization discrimination is higher than 20 dB.

II. TIGHTLY COUPLED REFLECTARRAY ELEMENT DESIGN

A. ELEMENT DESIGN

The tightly coupled reflectarray element in [13] is consisted of a wideband dipole (bowtie dipole) and a pair of true-time-delay (TTD) lines. Following this design guideline, we use elliptical dipole and TTD lines as wideband array element and spatial phase distribution structure respectively. The configuration of the element is shown in Fig. 1. The dipole element is printed on both sides of the substrate with a TTD line connected to each dipole arm. The element is placed perpendicular to the ground plane.

Firstly, we choose suitable geometry of the elliptical dipole which in this design the long axis of the dipole is 0.11\(\lambda\) (\(\lambda\) is center frequency wavelength). The TTD line width is designed to match the impedance of the dipole. The distance between the element and ground plane is the main factor that decides the bandwidth and we optimize \(h_1\) to obtain maximum bandwidth. However, some of the elements require large spatial phase delay which means that the corresponding TTD line is longer than the distance between the elements and ground plane. So we open a hole on the ground to let the line go through and add a second ground plane. In tightly coupled phase array, the mutual coupling is achieved by compact configuration or inter-element capacitance. In this paper the coupling strength is controlled by adjusting the overlapping distance of the dipole arms. We investigate the element reflection phase versus frequency of different coupling capacitance (\(l_p\)) in Fig. 2. When the TTD line is relatively short (\(l = 1\)), the reflection phase hardly changes as \(l_p\) increases. When the TTD line is in a medium range (\(l = 13\)), with the same increment of \(l_p\), the delayed phase is mildly enlarged. When \(l\) reaches relatively big value (\(l = 20\)), the amount of delayed phase is increased greatly in lower frequency whilst staying nearly unchanged in higher frequency.

Eventually we optimize \(l_p\) as well as other parameters to obtain a maximum operating bandwidth. All parameters of the element are shown in table 1. Fig. 3 illustrates element reflection coefficients of different TTD line length. The fairly
The equivalent distance delay lines in 3 GHz, 4 GHz and 5 GHz have good linearity, and are close to the designed line \( d(l) \). But \( d_{2GHz}(l) \) gradually deviates from \( d(l) \) as \( l \) grows which means the phase error in 2 GHz is becoming larger. From section II we know that the overlapping distance \( l_p \) affects the reflection phase in lower frequency. As the coupling strength attenuates, the delayed phase diminishes. So we develop a variant-coupling-capacitance method in which we change the value of \( l_p \) of each element according to its position to attain a more linear equivalent distance delay. Using this method the gain in lower frequency can be improved without deteriorating higher frequency performance. The method is explained in detail below.

Regarding the invariant-coupling-capacitance TCDRA, the space between neighboring elements is invariant. So \( s_i \), the distance from \( e_i(x_i, y_i) \) to the center, is

\[
    s_i = \sqrt{x_i^2 + y_i^2}
\]

In this paper, we aim to improve the linearity of \( d_{2GHz}(l) \) to improve gain in 2 GHz. It is found that by decreasing \( l_p \) the amount of delayed phase is decreased in lower frequency while stays mainly unchanged in higher frequency. Thus, we let coupling distance \( l_p \) decreases as \( l \) increases. As a result, the delayed phase decreases and \( d_{2GHz}(l) \) becomes closer to the designed line \( d(l) \). The equation to calculate \( l_p \) of elements of different positions is shown below.

\[
    l_{p_{\text{new}}}(i) = -\frac{l_p \cdot l(i) - l_{\text{max}} \cdot l_p}{l_{\text{max}} - l_{\text{min}}}
\]

In (6), \( l(i) \) is the original TTD line length of \( e_i \), \( l_{\text{max}} \) is the maximum value of \( l \) which is 28mm, and \( l_p \) is the original coupling distance which is 1.5mm. We put the original value of \( l(i) \) into this equation, and then the new coupling parameter \( l_{p_{\text{new}}}(i) \) of each element \( e_i \) is attained. The updated distance between \( e_i \) and its neighboring element nearer to the center is

\[
    \text{interval}(i) = \text{gap} + 2a - l_{p_{\text{new}}}(i)
\]

The \( y \) coordinate of \( e_i \) is unchanged. The \( x \) coordinate, \( x'_i \), and the distance from \( e_i \) to the center, \( s'(i) \) are shown respectively

\[
    x'_i = \sum_{i=1}^{n} \text{interval}(i)
\]

\[
    s'(i) = \sqrt{(x'_i)^2 + y_i^2}
\]
In (8), \(n\) is the number of elements between \(e_i\) and the center element which is in the same row with \(e_i\). The updated equivalent distance delay for elements with variant coupling capacitance is shown in Fig. 5 in line with dots. Compared with the situation of fixed coupling capacitance, \(D_{3GHz}(l), D_{4GHz}(l), D_{5GHz}(l),\) and \(D(l)\) have little variation while \(D_{2GHz}(l)\) becomes closer to our designed line \(D(l)\) which means smaller phase error in 2 GHz but nearly invariable reflection phase in other frequencies. The phase error in 2 GHz before and after using VCC method is shown in Fig. 6. As can be seen, the phase error is reduced. Additionally, the phase delay line length of different elements in the VTCDRA is shown in Fig. 7.

### IV. FEED ANTENNA AND REFLECTARRAY DESIGN

#### A. FEED ANTENNA

In this paper, a log-periodic dipole array (LPDA) is employed as the feed antenna. Though phase center of this antenna is not as stable as it of horn antenna, the flat structure causes less blockage and is easier fabricate. The LPDA is printed on a substrate (Rogers RO4350B) with the thickness of 0.8mm. The antenna is fed by a coaxial cable connected to the left end. The LPDA scaling factor is calculated in (10). The number of elements is 20. The parameters of the feed antenna is shown in table 1.

\[
\tau = \frac{fl1}{fl2} = \frac{fw1}{fw2}
\]

(10)

As the phase center of the feed antenna changes along with frequency, we take phase centers of six different frequency points sampled equidistantly from 2.5 GHz to 5 GHz and average the coordinate to obtain the equivalent phase center. The coordinate of phase center is shown in table 2. The layout of LPDA is shown in Fig. 8. Results in Fig. 9 show that the simulated and measured \(|S_{11}|\) are both below \(-10\) dB in the frequency range of 2 GHz to 5 GHz.

#### B. REFLECTING SURFACE

We design two reflecting surface using traditional method and VCC method respectively. Both TCDRA and VTCDRA are consist of 21 \(\times\) 21 elements as shown in Fig. 10. From Fig. 10 (b) we can see that the VTCDRA has the shape of a lantern with marginally larger physical aperture area than...
the traditional TCDRA. We let F/D ratio equals 1. The side length of the reflectarray in Fig. 10 (a) is 350mm, so the distance between the equivalent phase center of feed antenna and reflecting surface is also 350mm. In order to control variables, the distance between the equivalent phase center of feed antenna and the reflecting surface of VTCDRA is kept the same. The physical aperture area of the VTCDRA is 120743mm$^2$ while the physical aperture area of the TCDDRA is 113360mm$^2$.

V. SIMULATION AND EXPERIMENT VERIFICATIONS

The reflectarray element was simulated using floquet mode and the reflectarray radiation results were obtained using full wave EM simulation. The measurement of the radiation patterns was carried out using nearfield measurement shown in Fig. 11. Simulation and measurement results of radiation patterns in both E plane and H plane are shown in Fig. 12. Good agreement in radiation patterns is observed between the simulation and measurement results. The cross polarization discrimination is larger than 20 dB across the entire band which is smaller than simulation. This is because the installation is not perfectly accurate, resulting that feed antenna polarization is not strictly parallel with the reflectarray polarization. The measured antenna gain are given in Fig. 13. The VTCDRA gain varies from 14.4 dBi to 22 dBi. In 2 GHz, the gain is larger than the traditional TCDRA’s by 3 dBi. Figure 13 also shows the measured aperture efficiencies of both TCDRA and VTCDRA. The VTCDRA aperture efficiency varies from 33.3% to 47.5%, peaking at 2.2 GHz. The aperture efficiency in the designed frequency, 2 GHz, is increased from 19.3% to 40.9%. The increment in other frequencies is due to the truncation effect in arrays. However, the increment in 2 GHz is 21.6% which is much higher than other frequency, which is able to demonstrate the effectiveness of the method. To state the good property of the proposed antenna, the performance of some recent wideband reflectarray antennas reported in the literature and the VTCDRA in this paper are summarized in table 3.

VI. CONCLUSION

In this paper, a tightly coupled dipole reflectarray antenna is presented. A variant-coupling-capacitance method is also
FIGURE 12. Radiation patterns of the VTCDRA.
proposed to improve the designed tightly coupled dipole reflectarray antenna gain in lower frequency by changing the coupling capacitance between elements according to their different positions in the reflecting surface. The traditional reflectarray and the modified reflectarray using variant-coupling-capacitance method are both studied and measured to verify the theory respectively. The two reflectarrays can both work from 2 GHz to 5 GHz. But the modified antenna gain is improved by 3 dB in 2 GHz with corresponding aperture efficiency increased by 21.6%.

REFERENCES


